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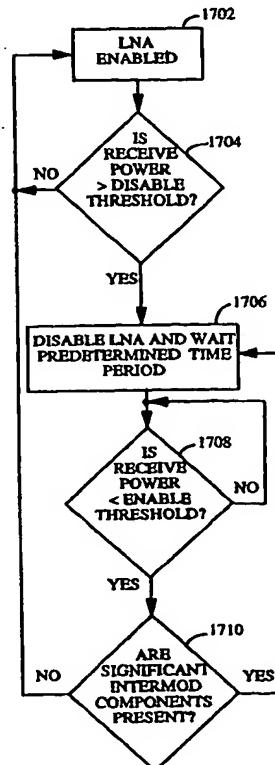
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(54) Title: METHOD AND APPARATUS FOR INCREASING RECEIVER IMMUNITY TO INTERFERENCE

(57) Abstract

A method for adjusting the gain of a receive circuit, thereby improving a receiver's immunity to interference. The circuit has an LNA which amplifies the received signal (1702). The receive signal power is controlled by enabling or disabling the LNA in response to the measured received signal power (1704). The received power level is periodically compared to a threshold (1704). When the received power level is greater than the threshold, the LNA is disabled (1706). The LNA is re-enabled when the received power level is less than the threshold (1708), and there are no significant intermodulation components detected (1710). The intermodulation components are detected by briefly enabling the LNA and detecting the resultant change in the measured signal power (1710). If the detected change is more than a predetermined amount, then there are significant intermodulation components present, and the LNA is not re-enabled (1706). Otherwise, there are not significant intermodulation components present, and the LNA is re-enabled (1702).



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METHOD AND APPARATUS FOR INCREASING RECEIVER IMMUNITY TO INTERFERENCE

BACKGROUND OF THE INVENTION

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I. FIELD OF THE INVENTION

The present invention relates to radio communications. More particularly, the present invention relates to improving a communication receiver's immunity to interference.

II. DESCRIPTION OF THE RELATED ART

There are presently multiple types of cellular radiotelephone systems operating. These systems include the advanced mobile phone system (AMPS) and the two digital cellular systems: time division multiple access (TDMA) and code division multiple access (CDMA). The digital cellular systems are being implemented to handle capacity problems that AMPS is experiencing.

All the cellular radiotelephone systems operate by having multiple antennas covering a geographic area. The antennas radiate into an area referred to in the art as a cell. The AMPS cells are separate and distinct from the CDMA cells. This makes it likely that the antenna for one system's cell may be located in a cell of another system. Likewise, within a particular system (AMPS, CDMA, and TDMA), there are two service providers within a given area. These providers often choose to place cells in different geographical locations from their competitor, hence there are situations where a radiotelephone on system 'A' might be far away from the nearest system 'A' cell while close to a system 'B' cell. This situation means that the desired receive signal will be weak in the presence of strong multi-tone interference.

This intermixing of system antennas can cause problems for a mobile radiotelephone that is registered in one system, such as the CDMA system, and travels near another system's antenna, such as an AMPS antenna. In this case, the signals from the AMPS antenna can interfere with the CDMA signals being received by the radiotelephone due to the proximity of the radiotelephone with the AMPS cell or the higher power of the AMPS forward link signal.

The multi-tone interference encountered by the radiotelephone from the AMPS signals creates distortion products or spurs. If these spurs fall in

the CDMA band used by the radiotelephone, they can degrade receiver and demodulator performance.

It is frequently the case in an AMPS system for the carriers (A and B bands) to 'jam' the competitor system unintentionally. The goal of the 5 cellular carrier is to provide a high signal to noise ratio for all the users of their system by placing cells close to the ground, or near their users, and radiating the FCC power limit for each AMPS channel. Unfortunately, this technique provides for better signal quality for the carrier's system at the expense of interfering with the competitor's system.

10 Intermodulation distortion, such as that caused by the above situations, is defined in terms of the peak spurious level generated by two or more tones injected into a receiver. Most frequently, the third-order distortion level is defined for a receiver in terms of a third-order input intercept point or IIP3. IIP3 is defined as the input power (in the form of two 15 tones) required to create third order distortion products equal to the input two tone power. As shown in FIG. 13, IIP3 can only be linearly extrapolated when a non-linear element, such as an amplifier, is below saturation.

20 As shown in FIG. 14, third-order distortion products occur when two tones are injected in a receiver. Tone #1 is at frequency f_1 at power level P_1 in dBm. Tone #2 is at frequency f_2 at power level P_2 in dBm. Typically P_2 is set to equal P_1 . Third-order distortion products will be created at frequencies 2 $f_1 - f_2$ and 2 $f_2 - f_1$ at power levels P_{12} and P_{21} respectively. If P_2 is set to equal P_1 , then spurious products should be equal, or P_{12} and P_{21} should be equal. Signal f_c is injected at power level P_c to show that the added 25 distortion is equal to a low level signal in this case. If there is a filter that filters out f_1 , f_2 and f_{21} after the distortion is created, the power at f_{12} will still interfere with the signal power at f_c . In example FIG. 14, for a CDMA application, the goal is that the intermod P_{12} should be equal to the signal power of -105 dBm for a total two tone power of -43 dBm, so the IIP3 must be 30 > -9 dBm.

As is well known in the art, IIP3 for a single non-linear element is defined as the following:

$$\text{IIP3} = + P_{\text{in}} \text{ (dBm)}$$

35 If $P_1 = P_2$, then $P_{\text{in}} = P_1 + 3 \text{ dB}$ or $P_2 + 3 \text{ dB}$ (dBm) and
 $\text{IM3} = P_1 - P_{12} = P_2 - P_{21} = P_2 - P_{12} = P_1 - P_{21} \text{ (dB)}$

For cascaded IIP3, where more non-linear elements are used, the equation is as follows:

$$\text{IIP3} = -10 \cdot \log_{10} [10(\text{Gain} - \text{element IIP3})/10 + 10(-\text{IIP3 of previous stages})/10]$$

where: Gain = gain to element input.

5 Therefore, one way to improve the cascaded IIP3 of a receiver is to lower the gain before the first non-linear element. In this case, the LNA and mixer limit IIP3. However, another quantity needs to be defined that sets the sensitivity or lowest receive signal level without interference. This quantity is referred to in the art as the noise figure (NF). If the gain of the receiver is
10 reduced to improve IIP3 (and interference immunity), the NF (and sensitivity to small desired signals) is degraded.

The Element NF is defined as the following:

$$\text{Element NF} = - ,$$

15 where: is the input signal to noise ratio in dB, and
is the output signal to noise ratio in dB.

For elements in cascade in a receiver, the equation is as follows:

$$\text{Cascaded NF} = 10 \cdot \log_{10} [10^{(\text{NFe}/10)} + \frac{10^{(\text{NFe}/10)} - 1}{10^{(\text{Gain}/10)}}],$$

20 where: NFe equals the noise figure of the element,
NFi equals the cascaded noise figure up to the element, and
Gain equals the running gain up to the element.

The 'best' cascaded NF can be achieved if the gain up to the element is maximized, this equation is in contradiction to the requirement for the 'best'
25 cascaded IIP3. For a given element by element and receiver NF and IIP3, there are a limited set of gain values for each element that meet all of the requirements.

Typically, a receiver is designed with NF and IIP3 as predefined constants, as both of these quantities set the receiver's dynamic range of
30 operation with and without interference. The gain, NF, & IIP3 of each device are optimized based on size, cost, thermal, quiescent and active element current consumption. In the case of a dual-mode CDMA/FM portable cellular receiver, the CDMA standard requires a 9 dB NF at minimum signal. In other words, for CDMA mode, the sensitivity requirement is a 0 dB S/N ratio at -104 dBm. For FM mode, the requirement is a 4 dB S/N ratio
35 at -116 dBm. In both cases, the requirements can be translated to a NF as follows:

NF = S (dBm) - Ntherm (dBm/Hz) - Signal BW (dB/Hz),
where S is the minimum signal power,
is the minimum signal to noise ratio,
Ntherm is the thermal noise floor (-174 dBm/Hz @ 290° K),
and Signal BW (dB/Hz) is the bandwidth of the signal.

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Therefore,

CDMA NF = -104 dBm - 0 dB - (- 174 dBm/Hz) - 61 dB/Hz = 9 dB,
10 FM NF = -116 dBm - 4 dB - (- 174 dBm/Hz) - 45 dB/Hz = 9 dB,
where -61 dBm/Hz is the noise bandwidth for a CDMA channel
-45 dBm/Hz is the noise bandwidth for a FM channel

15 However, the receiver's NF is only required when the signal is near
the minimum level and the IIP3 is only required in the presence of
interference or strong CDMA signals.

20 There are only two ways to provide coverage in the areas where the
carrier is creating strong interference. One solution is to employ the same
technique; i.e., co-locate their cells along with the competition's. Another
solution is to improve the immunity of a receiver to interference. One way
25 to improve the immunity is to increase the receiver current. This is not a
practical solution, however, for a portable radio that relies on battery power.
Increasing the current would drain the battery more rapidly, thereby
decreasing the talk and standby time of the radiotelephone. There is a
resulting need to minimize multi-tone interference in a radiotelephone
without impacting the current consumption.

SUMMARY OF THE INVENTION

30 The process of the present invention adjusts the gain of a receive
circuit, thereby improving a receiver's immunity to interference. The circuit
has an LNA which amplifies the received signal. The receive signal power
is controlled by enabling or disabling the LNA in response to the measured
received signal power. The received power level is periodically compared to
a threshold. When the received power level is greater than the threshold,
35 the LNA is disabled. The LNA is re-enabled when the received power level
is less than the threshold, and there are no significant intermodulation
components detected. The intermodulation components are detected by
briefly enabling the LNA and detecting the resultant change in the measured
signal power. If the detected change is more than a predetermined amount,

then there are significant intermodulation components present, and the LNA is not re-enabled. However, if the detected change is less than the predetermined amount, then there are not significant intermodulation components present, and the LNA is re-enabled.

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BRIEF DESCRIPTION OF THE DRAWINGS

FIG. 1 shows a block diagram of the apparatus of the present invention for increasing receiver immunity.

10 FIG. 2 shows a block diagram of another alternate embodiment of the present invention.

FIG. 3 shows a block diagram of another alternate embodiment of the present invention.

15 FIG. 4 shows a block diagram of another alternate embodiment of the present invention.

FIG. 5 shows a another plot of received RF input power versus carrier to noise ratio in accordance with the embodiment of FIG. 7.

FIG. 6 shows a plot of receive RF input power versus carrier to noise ratio in accordance with the embodiment of FIG. 8.

20 FIG. 7 shows a block diagram of another alternate embodiment of the present invention.

FIG. 8 shows a plot of interference power vs. signal power without using the apparatus of the present invention.

25 FIG. 9 shows a plot of interference power vs. signal power in accordance with the alternate embodiments of the apparatus of the present invention.

FIG. 10 shows a block diagram of an alternate embodiment of the present invention.

30 FIG. 11 shows a block diagram of another alternate embodiment of the present invention.

FIG. 12 shows a block diagram of another alternate embodiment of the present invention.

FIG. 13 shows a plot of non-linear transfer characteristics and distortion measurement.

35 FIG. 14 shows a spectral description of distortion products.

FIG. 15 shows a block diagram of a method for detecting the power of a received signal in accordance with the present invention.

FIG. 16 shows a flow chart of the gain control process of the present invention.

FIG. 17 shows a flow chart of an alternate embodiment of the gain control process of the present invention.

DETAILED DESCRIPTION OF THE PREFERRED EMBODIMENTS

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It is an objective of the present invention to vary the receiver NF and IIP3 for enhancing the IIP3 (or interference immunity) without compromising NF when necessary. This performance 'enhancement' is 10 accomplished by varying the gain of the first active element in the receiver. The gain can be varied by varying the gain of the LNA over a continuous range or switching out the low noise amplifier with bypass switches.

A block diagram of the preferred embodiment of the present invention is illustrated in FIG. 1. This embodiment involves adjusting the 15 LNA 115 gain on a continuous basis using adjustable gain control (AGC) 110 at the receiver front end. The continuous AGC 110 at the front end also provides a linearity benefit at a minimum RF input level while the AGC 120 on the transmit side may reduce the IF AGC 125 and 130 requirements.

This embodiment detects the power output from the LNA 115. The 20 power detector 105 measures both the signal power and the jammer power together at RF. Using this embodiment, the power detector 105 can continuously decrease the LNA 115 gain at a lower received power than the -65 dBm of the subsequent "switched gain" embodiments of FIGs. 7, 10, 11 and 12.

The preferred embodiment operates by the power detector 105 detecting the received signal and jammer power at RF. This detected power goes through a loop filter and is used to adjust the receive AGC 110, thereby 25 adjusting the intercept point of the receive components. The gain is decreased as the measured power increases and the gain is increased as the measured power decreases. This embodiment could also combine the LNA 115 and the AGC 110 to form a variable gain LNA, thus eliminating the need for the separate AGC 110 block. The power of the transmit AGC 120, located before the power amplifier 150, is adjusted in the same way as the receive AGC 110 in order to maintain the overall TX power level.

35 AGC amplifiers 125 and 130 are also located after the mixers 135 and 140 in order to adjust the gain after the jammers have been filtered out by the bandpass filter 145. These AGC amplifiers 125 and 130 perform the normal CDMA AGC function of open loop power control, closed loop power control, and compensation. These IF AGCs 125 and 130 are required due to

the wide dynamic range requirements for CDMA. Typically, these AGCs 125 and 130 have greater than 80 dB of gain range. The receive and transmit AGC 125 and 130 after the mixers are adjusted by another power detector 150 that measures the total power after the received signal is downconverted.

- 5 The power detector 150 adjusts the AGCs 125 and 130 gain downward as the downconverted signal's power increases and adjusts the AGCs 125 and 130 gain upward as the downconverted signal's power decreases.

In the preferred embodiment, the received signals are in the frequency band of 869-894 MHz. The transmitted signals are in the frequency 10 band of 824-849 MHz. Alternate embodiments use different frequencies.

The plot illustrated in FIG. 5 shows the benefit of this AGC approach. The left hand y-axis shows the carrier over noise ratio versus receive input power parameterized by the jammer level. The right hand y-axis shows the 15 total jammer power required for a constant C/J as a function of received input power. When the jammer is not present (-100 dBm), the radio operates as though there is no RF AGC. As the jammer is increased, the C/N is decreased, but the effective linearity is also increased. In this example, the RF dynamic range is 30 dB and the threshold, where the RF AGC becomes active, is at the point the jammer power is greater than -25 dBm.

20 An alternate embodiment of the continuous gain adjustment is illustrated in FIG. 2. This embodiment first filters out the jammers with the bandpass filter 205 before the power detector 210 determines the power level of the downconverted signal. A threshold detector 225 determines when the 25 signal power level reaches a certain point, -105 dBm in this embodiment, and then adjusts the AGCs 230 and 235 gain down when the signal power exceeds that power level. The AGCs 230 and 235 gain is adjusted upward when the signal power level goes below this threshold. The gain of AGCs 215 and 220 after the mixers 240 and 245 is adjusted continuously without 30 checking for a predetermined threshold of power, performing the normal CDMA AGC power control.

The plot of this embodiment is illustrated in FIG. 6. When the threshold is set at -105 dBm, the minimum receive RF level, the C/N does not increase as quickly as the case where there is no RF AGC. The advantage 35 of this embodiment is that the linearity benefit begins at a very low RF input power, no receive RF power detector is needed, and the AGC loop detects signal power only. Hence, the AGC loop is a simpler design than detecting at RF power.

Still another embodiment of the present invention is illustrated in FIG. 3. This embodiment operates similarly to the embodiment of FIG. 1.

The only difference being the placement of the AGC 301 prior to the LNA 305 in the receive path.

Yet another embodiment of the present invention is illustrated in FIG. 4. This embodiment uses an attenuator 405 between the antenna 410 and the duplexer 415. The attenuation is controlled by the power detector 420 after the LNA 425. The power detector 420 measures the received signal and jammer power, filters it, and compares it to a predetermined threshold. In this embodiment, the threshold is -25 dBm. When the combined signal and jammer power reaches this threshold, the attenuation caused by the attenuator 405 is increased. This adjustment can be either in digital fixed steps or continuously adjusted. The AGC 430 and 435 after the mixers 440 and 445 are adjusted in the same manner as the FIG. 1 preferred embodiment.

An alternate embodiment of the apparatus of the present invention is illustrated in FIG. 7. This embodiment uses switches 701 and 702 to alter the front end gain. The actual switching level depends on the signal to noise requirements as a function of the signal level, or noise figure, for a particular CDMA radiotelephone design. The present invention can be used in an AMPS radiotelephone, however the switching characteristics will be changed to accommodate a different operating point.

This embodiment is comprised of an antenna 725 that receives and transmits radio signals. Receive and transmit paths in the radio are coupled to the antenna 725 through a duplexer 720 that separates the received signals from the transmitted signals.

A received signal is input to an LNA 703 that is coupled between two switches 701 and 702. One switch 701 couples the LNA 703 to the duplexer 720 and the second switch 702 couples the LNA 703 to a band-pass filter 704. In the preferred embodiment, the switches 701 and 702 are single-pole double-throw gallium arsenide switches.

The LNA 703 is coupled to one pole of each switch such that when both switches 701 and 702 are switched to those poles, the received signal is coupled to the LNA 703 and the amplified signal from the LNA 703 is output to the band-pass filter 704. The band-pass filter 704 in this embodiment has a frequency band of 869-894 MHz. Alternate embodiments use different bands depending on the frequencies of the signals being received.

A bypass path 730 is coupled to the other pole of each switch. When the switches 701 and 702 are switched to their other poles, the received signal from the duplexer 720 bypasses the LNA 703 and is conducted directly to the

band-pass filter 704. In this embodiment, these switches 701 and 702 are controlled by the radiotelephone's microcontroller 740. In an alternate embodiment, a separate controller is used to control the positions of these switches. Additionally, in other embodiments, attenuation (not shown) 5 may be provided along bypass path 730 if desired.

After the band-pass filter 704 has filtered the received signal, the filtered signal is downconverted to a lower intermediate frequency (IF) for use by the rest of the radio. The down-conversion is done by mixing 705 the received signal with another signal having a frequency set by a phase locked 10 loop 707 driving a voltage controlled oscillator 706. This signal is amplified 750 before being input to the mixer 705.

The downconverted signal from the mixer 705 is input to the back end AGCs 708 and 709. These AGCs 708 and 709 are used by the radiotelephone for closed loop power control, as is already well known in 15 the art.

In the process of the present invention, the microcontroller 740 monitors the power of the received signal. When the power exceeds -65 dBm, the microcontroller 740 instructs the switches 701 and 702 to switch to the bypass position, thus coupling the received signal directly to the 20 bandpass filter 704. By bypassing the LNA 703 gain, the intercept point for the receiver is increased proportionally by the reduction in gain in dB. Alternate embodiments use other circuitry and methods to monitor the power of the received signal.

An alternate embodiment of the process of the present invention 25 continuously adjusts the front end gain. This embodiment uses a lower power threshold such as -25 dBm.

The plots of FIGs. 8 and 9 illustrate the benefits of the switchable gain 30 embodiments of the present invention illustrated in FIGs. 7, 10, 11 and 12. FIG. 8 illustrates a plot of interference power versus radio frequency (RF) signal power for a typical radio that is not using the switchable gain apparatus. This plot shows that the maximum interference level is limited to the receiver input compression point at -10.5 dBm. Both the single and dual tone power curves are shown.

The plot of FIG. 9 shows the interference power received by the radio 35 versus the radio frequency signal power received by the radio using the switchable gain method and apparatus of the present invention. It can be seen that at the -65 dBm point of the graph, the switches are switched to bypass the LNA gain thus allowing a greater interference power to be

tolerated without affecting the RF signal power. Both the single tone and two tone power curves are shown.

Another alternate embodiment of the apparatus of the present invention is illustrated in FIG. 10. This embodiment uses a single-pole single-throw switch 1001. In this embodiment, the switch 1001 is switched to the bypass path 1010 by the controller 1020 when the received signal power reaches -65 dBm. This effectively shorts out the LNA 1002 gain, thus coupling the received signal directly to the band-pass filter 1003.

Yet another alternate embodiment of the apparatus of the present invention is illustrated in FIG. 11. This embodiment uses a single-pole single-throw switch 1105 that, when closed, shorts the input of the LNA 1110 to ground through a resistor 1101. This creates an impedance mismatch at the input causing the signal to attenuate, thus reducing the gain caused by the LNA 1110. As in the above embodiments, the switch 1105 is closed when the input signal power reaches -65 dBm. The resistance required for the resistor 1101 is dependent on the amount of attenuation desired. This resistance will be different for different LNA's in alternate embodiments.

Still another embodiment of the apparatus of the present invention is illustrated in FIG. 12. This embodiment uses a single-pole double-throw switch 1201 at the output of the LNA 1205. The LNA 1205 is connected to one pole of the switch 1201 and a bypass path 1210 is connected to the other pole. The input to the bypass path 1210 is connected to the input of the LNA 1205. When the power level of the received RF signal reaches -65 dBm, the switch 1201 is thrown from the position coupling the LNA 1205 to the band-pass filter 1220 to the bypass path 1210. This couples the signal directly to the band-pass filter 1220, bypassing the gain of the LNA 1205.

In all of the above embodiments, the LNA can be powered down at the same time that it is bypassed by the switch or switches. This can be accomplished by connecting the LNA's power pin to a switch that is also controlled by the controller. Once the LNA is bypassed and is no longer used, power can be removed. This reduces the power consumption of the radio, thus increasing the talk and standby time for which the battery can be used.

In another embodiment of the present invention, E_c/I_o detection is used to determine when to adjust the front end gain. Additional embodiments use other quality measurements, such as E_b/I_o .

These ratios are quality measurements for digital communications system performance. The E_b/I_o ratio expresses the energy per bit to the total interference spectral density of the channel while the E_c/I_o ratio expresses the energy per CDMA chip relative to the total interference spectral density.

E_b/I_o can be considered a metric that characterizes the performance of one communication system over another; the smaller the required E_b/I_o the more efficient is the system modulation and detection process for a given probability of error. Given that E_c/I_o and received signal strength are readily available, the microcontroller can detect the presence of strong interference as a drop in E_c/I_o while the AGC detector detects the increased interference. The microcontroller can lower the front end gain to improve interference immunity which would improve E_c/I_o and lower the distortion products falling within the signal bandwidth.

When the signal quality goes above the E_b/I_o or E_c/I_o threshold, the front end gain is reduced. The gain adjustment can be accomplished using either the continuous adjustment method or the amplifier switching method, both described above.

Still another embodiment, illustrated in FIG. 15, would be to detect the signal power at IF or baseband instead of the combination of the signal and jammer power at RF. This approach is simpler in that there is only one power detector and AGC control loop.

FIG. 15 illustrates a block diagram of the alternate method of detecting the power of the received signal. The signal is first downconverted to baseband frequency 1501. This analog signal is then converted to a digital signal 1505 for further baseband processing including determining the received signal strength. The chip correlator 1510 determines the energy per chip with respect to the energy of all the non-coherent components. This information, along with the received signal strength indicator (RSSI) is used by the processor 1515 to determine the amount of gain adjustment for both the receive 1520 and transmit 1530 power.

Since the received signal power measurement includes both the signal and jammer power, the receive gain is increased only when both the signal level and the energy per chip drops. Since the RSSI is being changed, the transmit power must also be changed to compensate, thus enabling the open loop power control to operate properly. Thus, the processor adjusts the transmit gain whenever the receive gain is adjusted.

Other embodiments use erasures or signal power to control the variable gain AGC. Additional embodiments, instead of controlling both transmit and receive power, only control receiver power.

A process for controlling the gain of the above embodiments is illustrated in FIG. 16. This process is based on the relationship illustrated in the graph of FIG. 13. In FIG. 13, one can see that as the interference input power increases along the X axis, the intermodulation products (the lower

curve) increase faster than the interference power. Therefore, X dB of attenuation applied at the input will result in a decrease of the IM3 intermodulation products by $3 \times X$ dB if interference is present at the receiver input.

5 Typically, intermodulation products don't fall into the IF section of the radio due to their low power. Intermodulation products outside of the IF section of the radio do not cause receiver performance problems. Thus, adjustment of the receiver gain is only necessary if the intermodulation products are of sufficient power to affect the IF signal.

10 Referring to FIG. 16, the process of the present invention first adjusts the input gain 1601. In the preferred embodiment, this gain adjustment is 3 dB. However, other embodiments can use other values of gain adjustment, such as the range of 1 dB - 6 dB. The receiver processing is then used to measure the change in the power of the received signal 1605. In the 15 preferred embodiment, the automatic gain control processing detects the IF signal power change. It is understood that measurement of the change in received signal power may be accomplished at the RF or baseband stages of the receiver as well.

20 If the signal power changes by approximately 3 dB, the CDMA signal is greater than the noise floor and there are no intermodulation products that might cause problems. Additional gain adjustment is not needed in this case, but increasing the gain will improve receiver sensitivity. IF signal power changes of approximately (3 ± 0.5) dB are still considered to be 3 dB.

25 If the IF signal power changes by less than 3 dB 1610, the CDMA signal is less than the noise floor or there are no intermodulation products that might cause problems. In this case, the AGC is only seeing a small CDMA signal and noise. Therefore, it is necessary to increase the receiver circuit gain 1615 and thus increase the sensitivity of the receiver.

30 If the IF signal power changes by more than 3 dB, the intermodulation products are causing enough of a problem that additional gain adjustment is necessary 1620. In the preferred embodiment, if the input gain was changed by 3 dB the intermodulation products will change by 9 dB when large interference is present. In this case, the average gain may be decreased by a small amount (e.g., 3 dB) until the process of the present invention 35 determines that the intermodulation products are reduced to an acceptable level.

The process of the present invention can be used continuously, checking for intermodulation products at a low rate. This rate is ten times per second in the preferred embodiment. Other embodiments use the

process once per frame cycle. Still other embodiments use the process at other rates, such as upon detection of a significant error on the forward link.

An alternate embodiment of the method of the present invention is illustrated in FIG. 17. In this alternate embodiment, a "hold" time is introduced. As with the embodiment of FIG. 16, this alternate embodiment may be used to control the gain of any of the previous circuits described herein, using any of the previously disclosed power detectors, LNA's and controllers. Furthermore, it should be noted that although this alternate embodiment is disclosed with reference to an LNA, it is equally applicable to other types of amplifiers, whether fixed or variable gain.

The process begins in block 1702 with the LNA being "enabled", i.e. with the LNA amplifying the received RF signal. At decision diamond 1704, it is determined whether the received power is greater than a disable threshold, as was previously discussed with reference to FIGs. 1-4. If the received power is not greater than the disable threshold, then the process returns to block 1702.

The process remains with the LNA enabled until it is determined in decision diamond 1704 that the received power is indeed greater than the disable threshold, and the process moves to block 1706 where the LNA is "disabled", i.e. prevented from amplifying the received RF signal, for a predetermined time period. This predetermined time period may be referred to as a "hold" time which is desirable in order to limit the rate of switching the LNA in and out. By adding this "hold" time, the receive automatic gain control loops (see FIGs. 1-4 and 15) may be kept stable.

After the expiration of the predetermined time period (i.e. the hold time) of block 1706, the received power is again measured, and this time compared with an enable threshold in decision diamond 1708. In the preferred embodiment, the enable threshold of decision diamond 1708 is less than the disable threshold of decision diamond 1704, thereby providing hysteresis. However, this is not strictly required.

If the received power is greater than the enable threshold, then the received power is still too high, and the LNA remains disabled until the received power is less than the enable threshold. When the received power is less than the enable threshold as determined in decision diamond 1708, then the process continues to decision diamond 1710 where it is determined whether significant intermodulation components are present. This determination is preferably made by switching in the LNA for a brief period and measuring the "shift" (i.e. the amount of AGC compensation) in the receive automatic gain control loops. As was discussed with reference to

FIG. 16, the presence of significant intermodulation components would cause the received signal power to increase more than it would in the presence of the desired signal only. This extra increase in received signal power would cause the receive automatic gain control loops to provide a greater gain control signal to the AGC amplifiers.

If there are significant intermodulation components present as determined in decision diamond 1710, then the LNA is not re-enabled, but rather the process returns to block 1706 where the LNA remains disabled for the predetermined time period. However, if there are no significant intermodulation products present, then the front end gain may be increased to improve the receiver performance by re-enabling the LNA and returning to block 1702.

In summary, the method of the present invention enables a mobile radio to travel near antennas of different systems while increasing the radio's resistance to radio frequency interference from the other system. By decreasing the front end gain, the intercept point of the radio's receive circuitry increases so that the spurs from the other system's signals will not cause performance degradation of the receiver and demodulator.

The previous description of the preferred embodiments is provided to enable any person skilled in the art to make or use the present invention. The various modifications to these embodiments will be readily apparent to those skilled in the art, and the generic principles defined herein may be applied to other embodiments without the use of the inventive faculty. Thus, the present invention is not intended to be limited to the embodiments shown herein but is to be accorded the widest scope consistent with the principles and novel features disclosed herein.

WE CLAIM:

CLAIMS

1. A method for adjusting the gain of a circuit, the circuit having
2 an amplifier and receiving a signal having power, the method comprising
the steps of:

- 4 measuring power of said signal;
- 6 comparing said measured power of said signal with a first threshold;
- 8 decreasing a gain of said amplifier for a predetermined time period if
said measured signal power is greater than said first threshold;
- 10 remeasuring power of said signal;
comparing said remeasured power of said signal with a second
threshold;
- 12 varying said gain of said amplifier;
- 14 detecting a change in said signal power;
increasing said gain of said amplifier if said remeasured power of said
signal is less than said second threshold and said detected change is less than
a predetermined amount.

2. The method of claim 1 wherein said amplifier has a high gain
setting and a low gain setting, and wherein said step of decreasing said gain
includes switching said amplifier to said low gain setting, and wherein said
step of increasing said gain includes switching said amplifier to said high
gain setting.

3. The method of claim 2 further comprising the steps of
switching said amplifier to said low gain setting for said predetermined time
period if said remeasured power of said signal is not less than said second
threshold or said detected change is not less than said predetermined
amount.

4. The method of claim 3 wherein said first threshold is greater
than said second threshold.

5. The method of claim 3 wherein said amplifier is a fixed gain
amplifier and said low gain setting is substantially equal to zero gain.

6. A method for varying a gain of a receive circuit having a fixed
gain amplifier, the method comprising the steps of:
receiving a signal;
4 amplifying said received signal with said fixed gain amplifier;

- measuring an amplified signal power of said amplified signal;
- 6 comparing said measured amplified signal power with a first threshold;
- 8 preventing said fixed gain amplifier from amplifying said received signal for a first predetermined period if said measured signal power is
- 10 greater than said first threshold;
- 12 measuring a non-amplified signal power of said received signal after said first predetermined period has elapsed;
- 14 comparing said measured non-amplified signal power with a second threshold;
- 16 re-amplifying said received signal with said amplifier for a second predetermined period;
- 18 measuring a re-amplified signal power of said re-amplified signal;
- 20 detecting a difference between said measured non-amplified signal power and said re-amplified signal power; and
- 22 repeating said amplifying step if said measured non-amplified signal power is less than a second threshold and said detected difference is less than a predetermined amount.

7. The method of claim 6 further comprising the step of

2 preventing said fixed gain amplifier from amplifying said received signal for said first predetermined period if said measured non-amplified signal power

4 is not less than said second threshold or said detected difference is not less than said predetermined amount.

8. The method of claim 7 wherein said first threshold is greater

2 than said second threshold.

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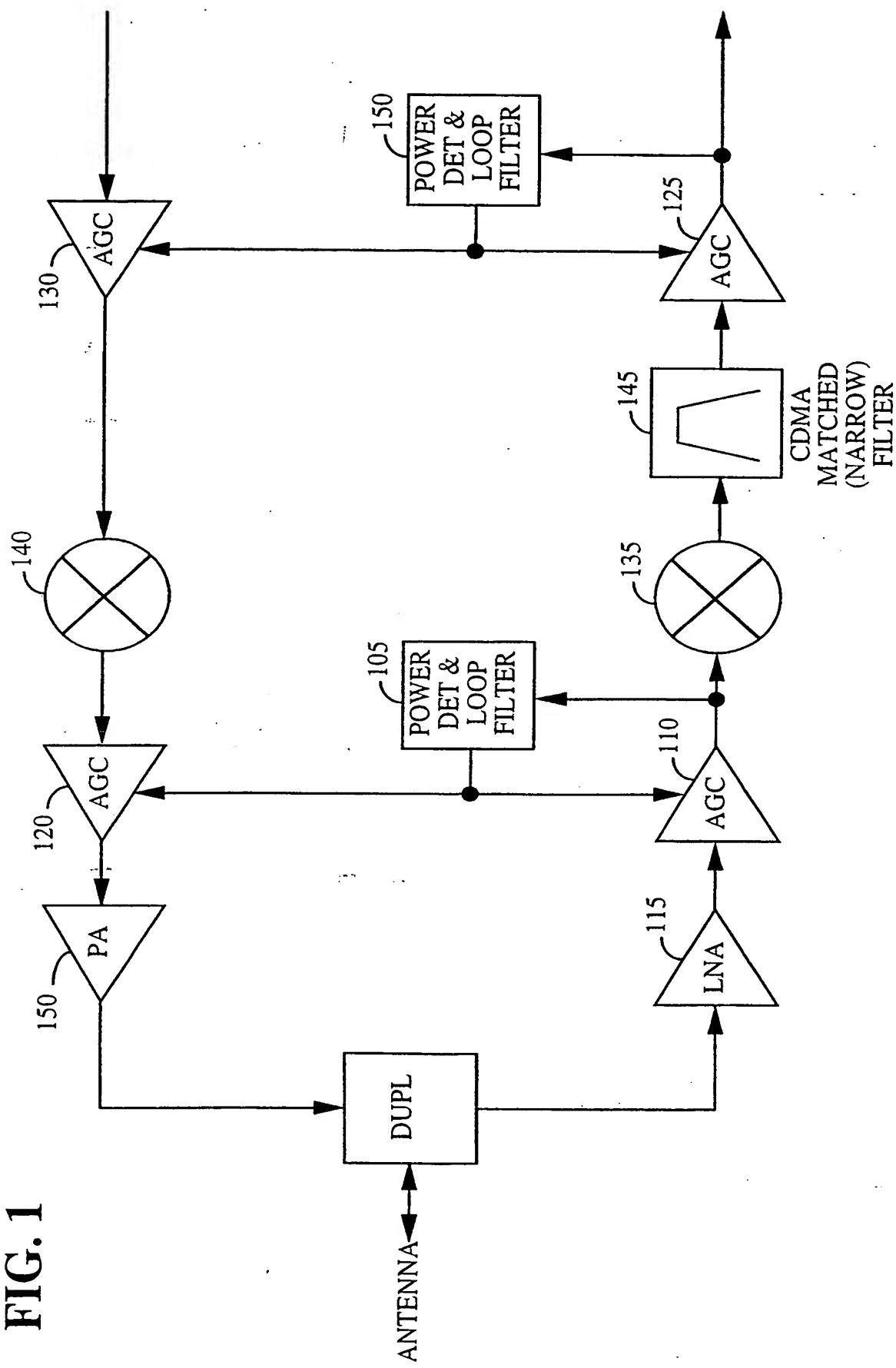


FIG. 1

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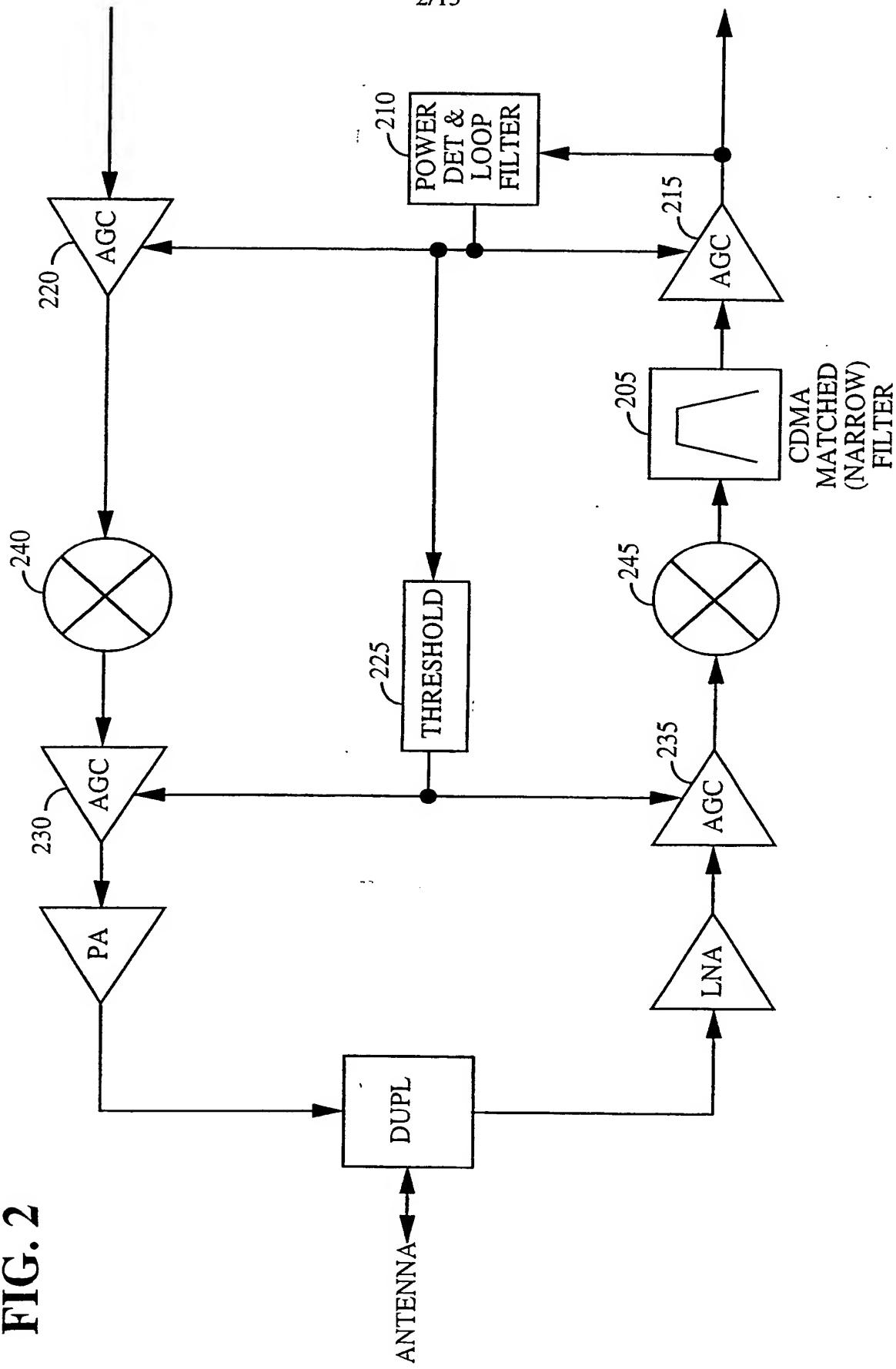


FIG. 2

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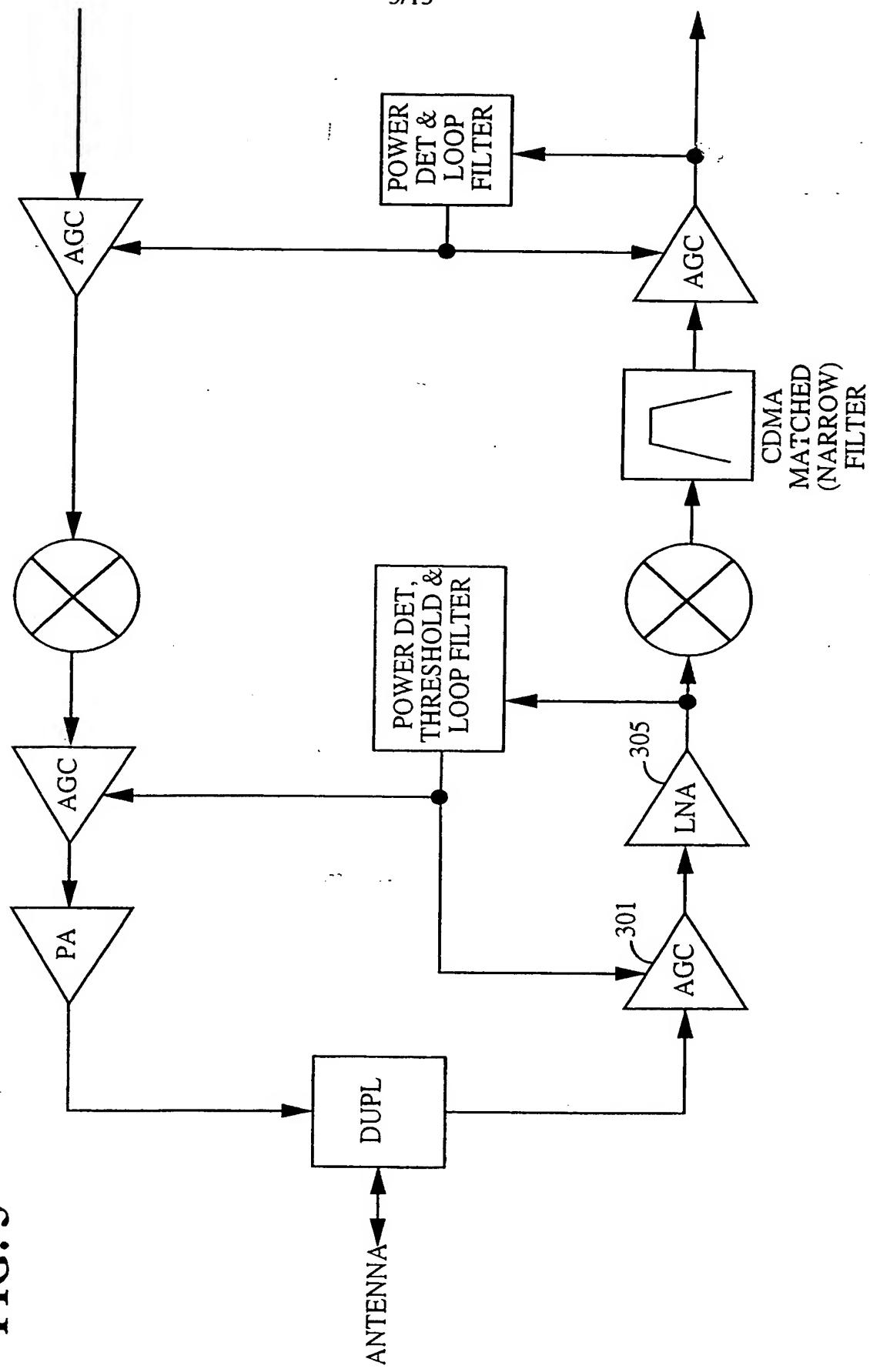


FIG. 3

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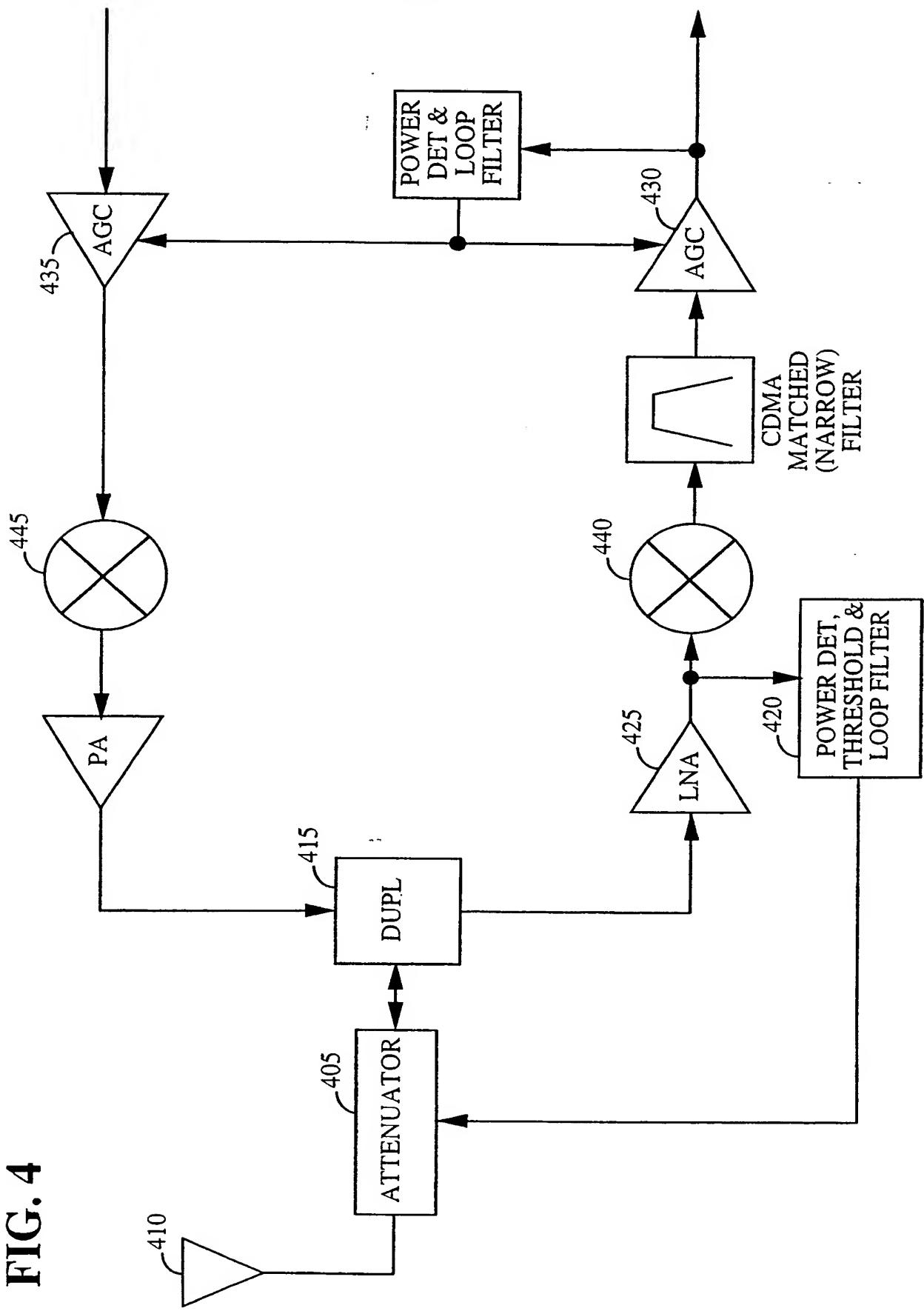


FIG. 4

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FIG. 5

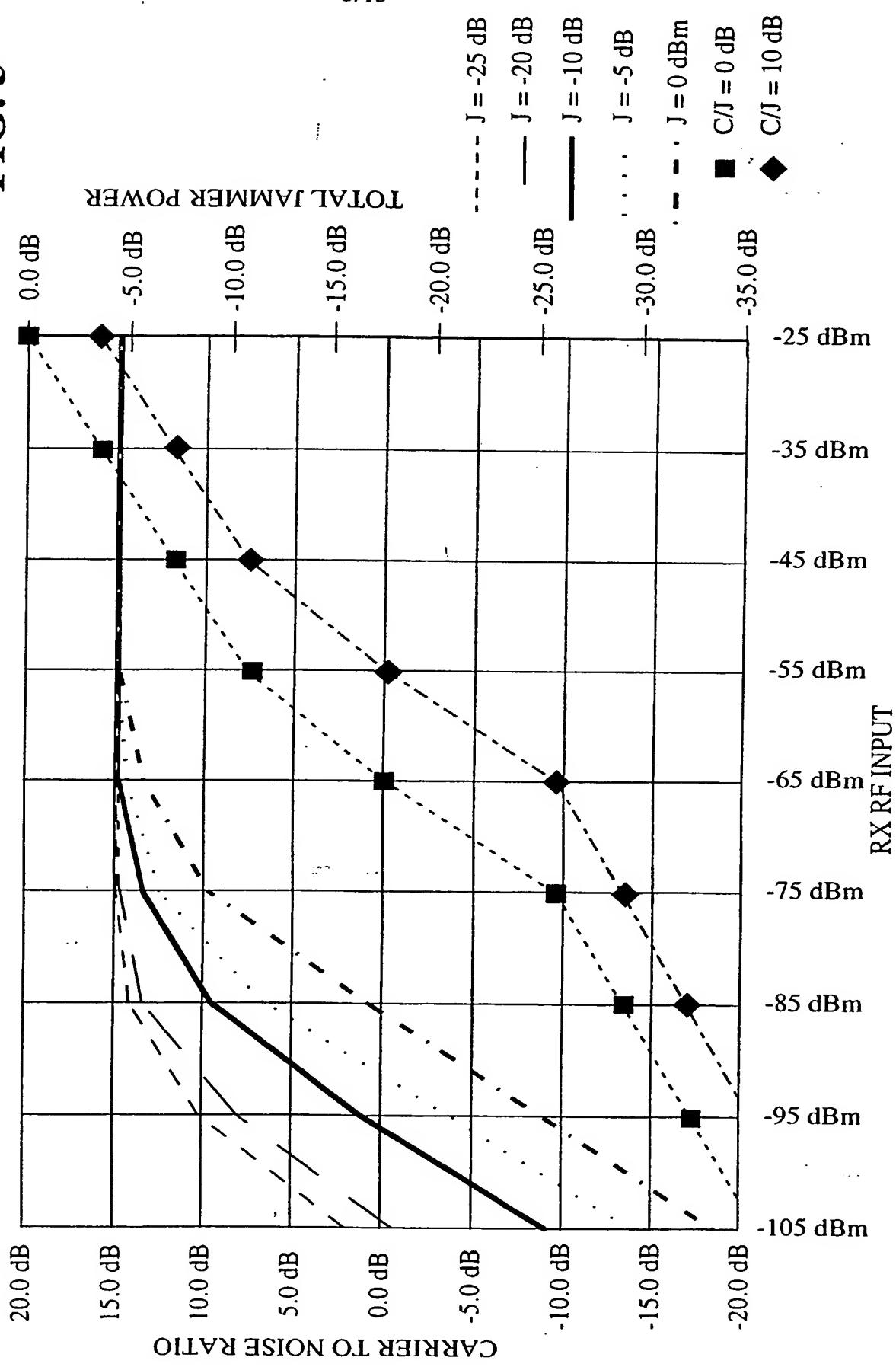
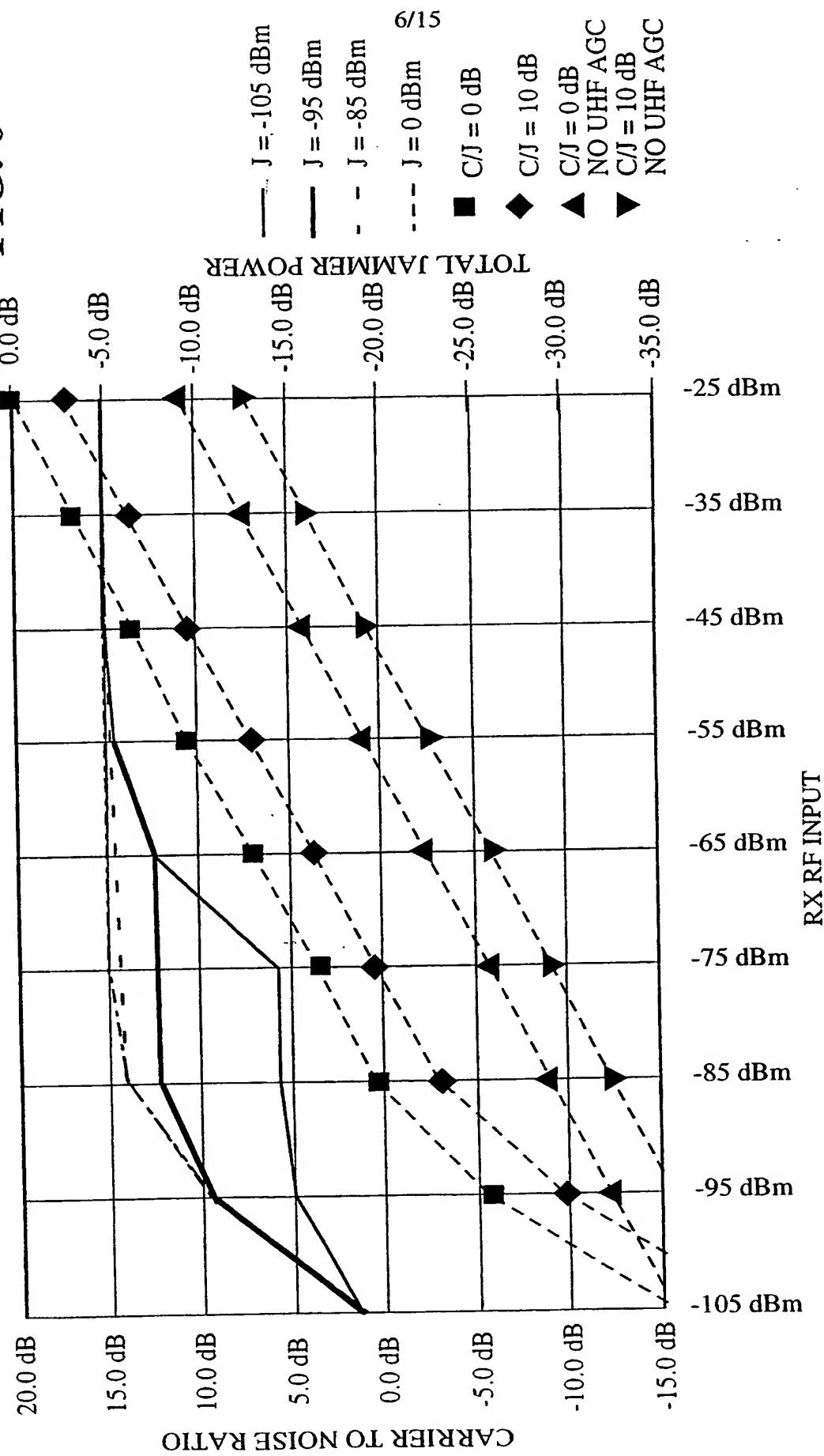
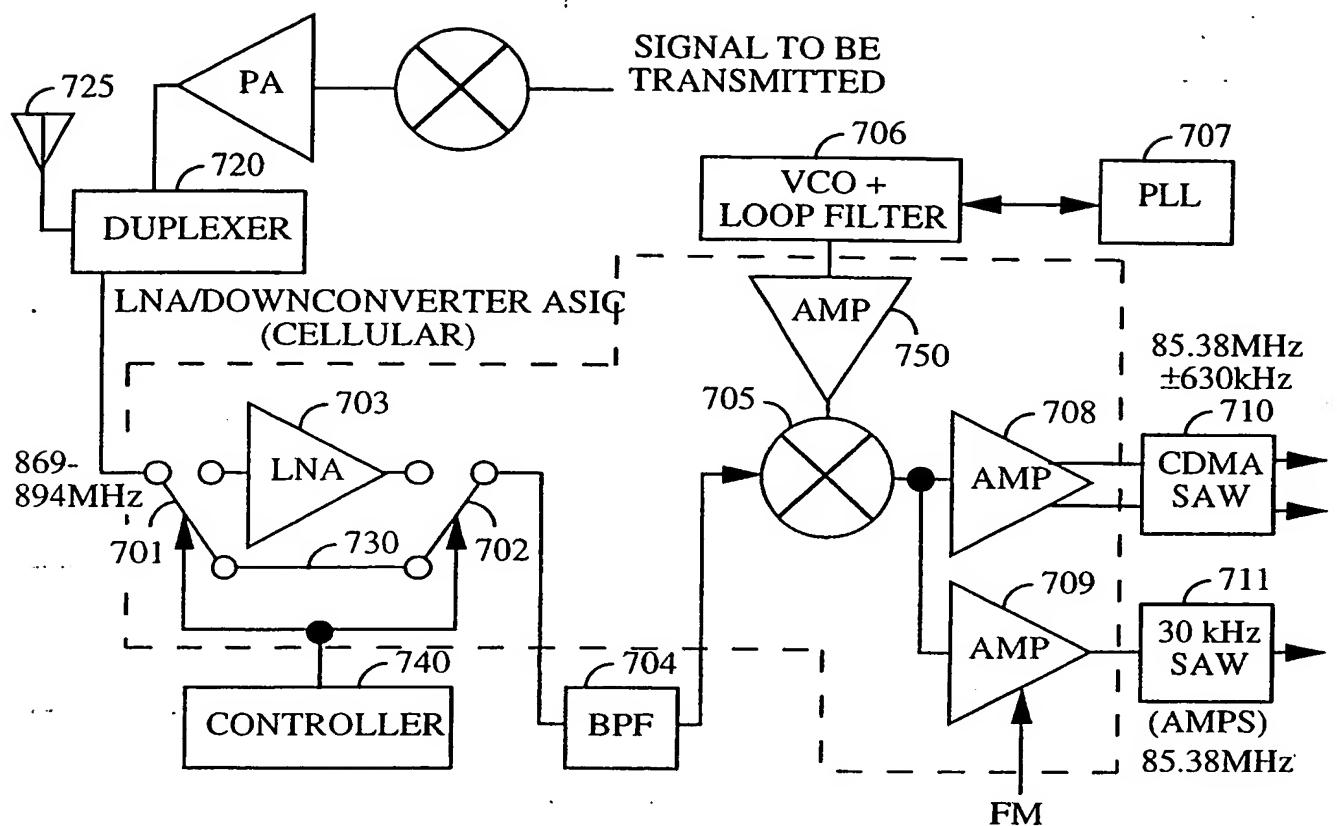
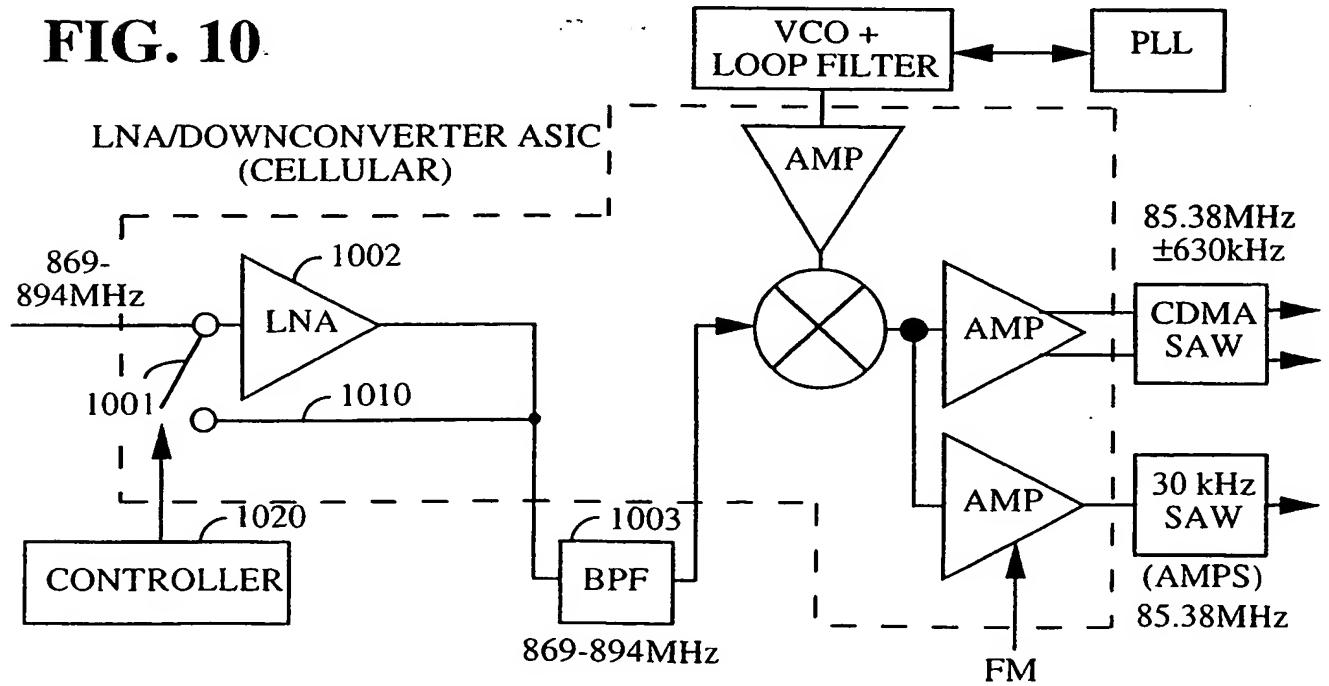


FIG. 6



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FIG. 7**FIG. 10**

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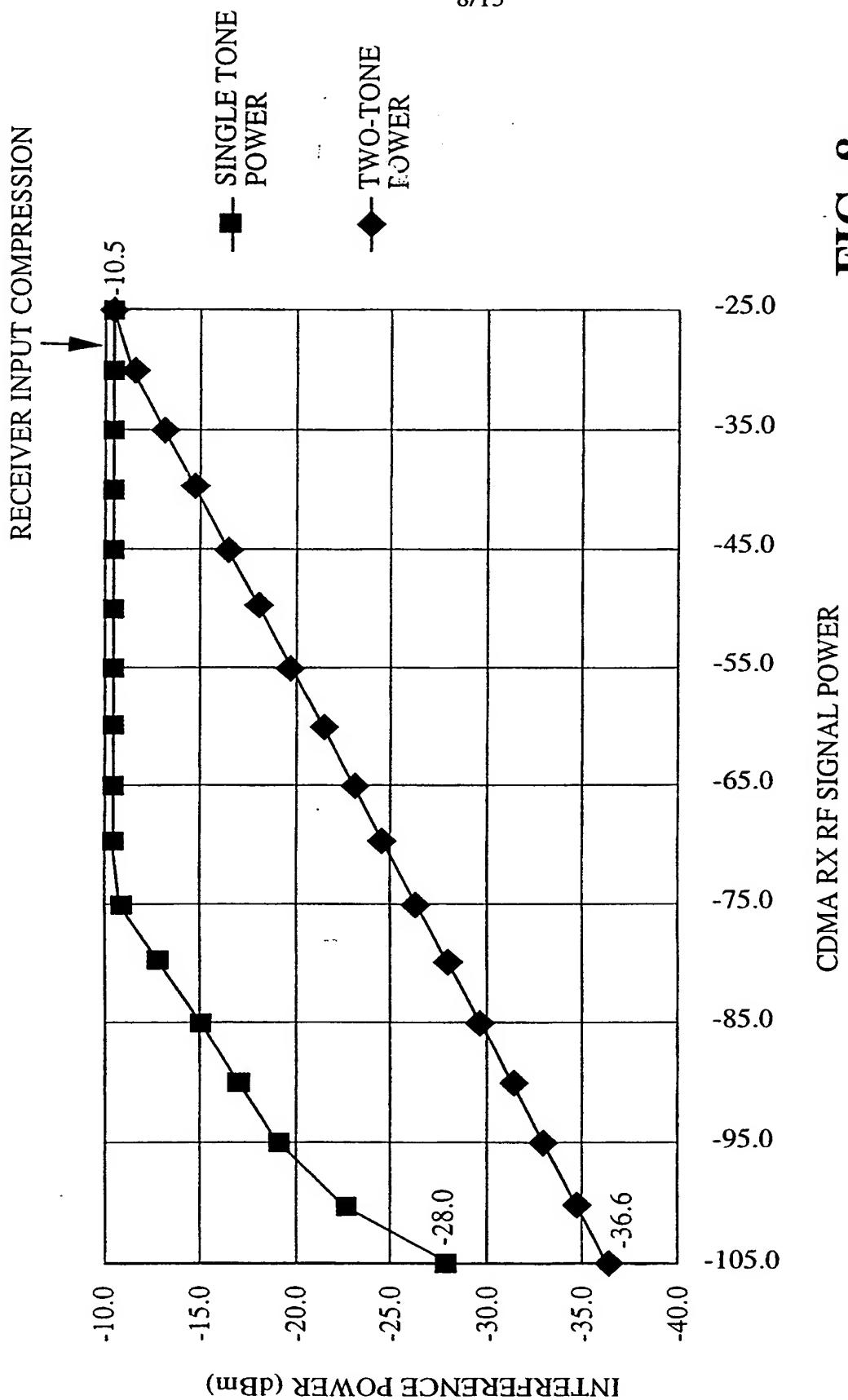


FIG. 8

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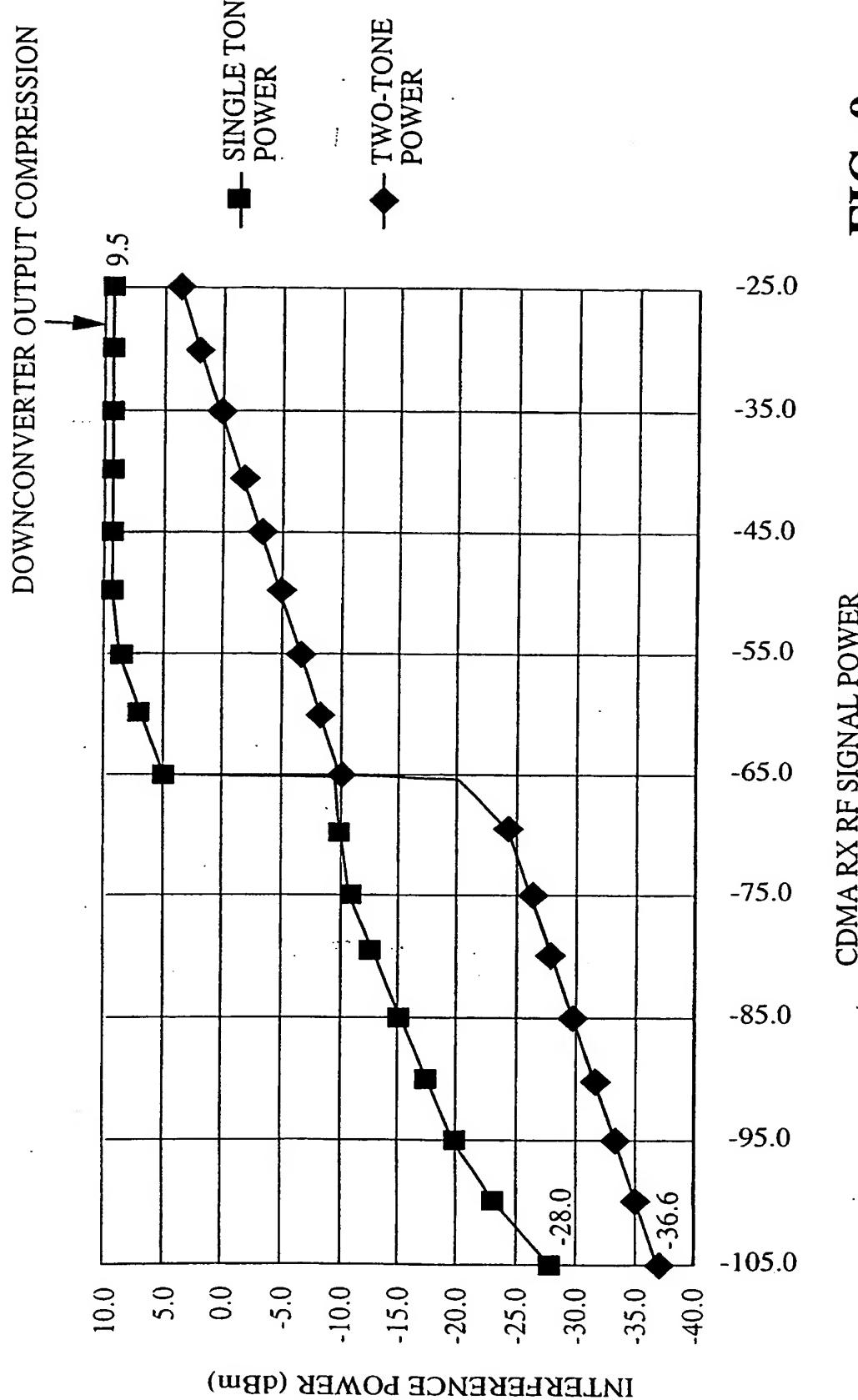
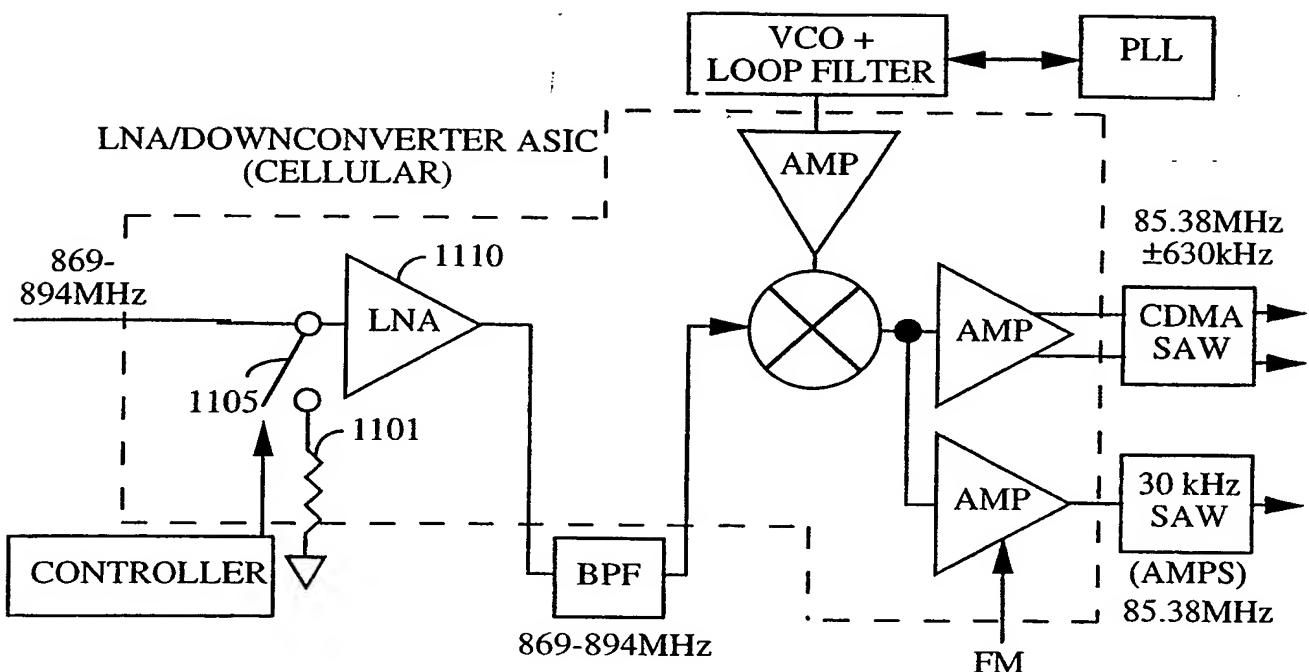
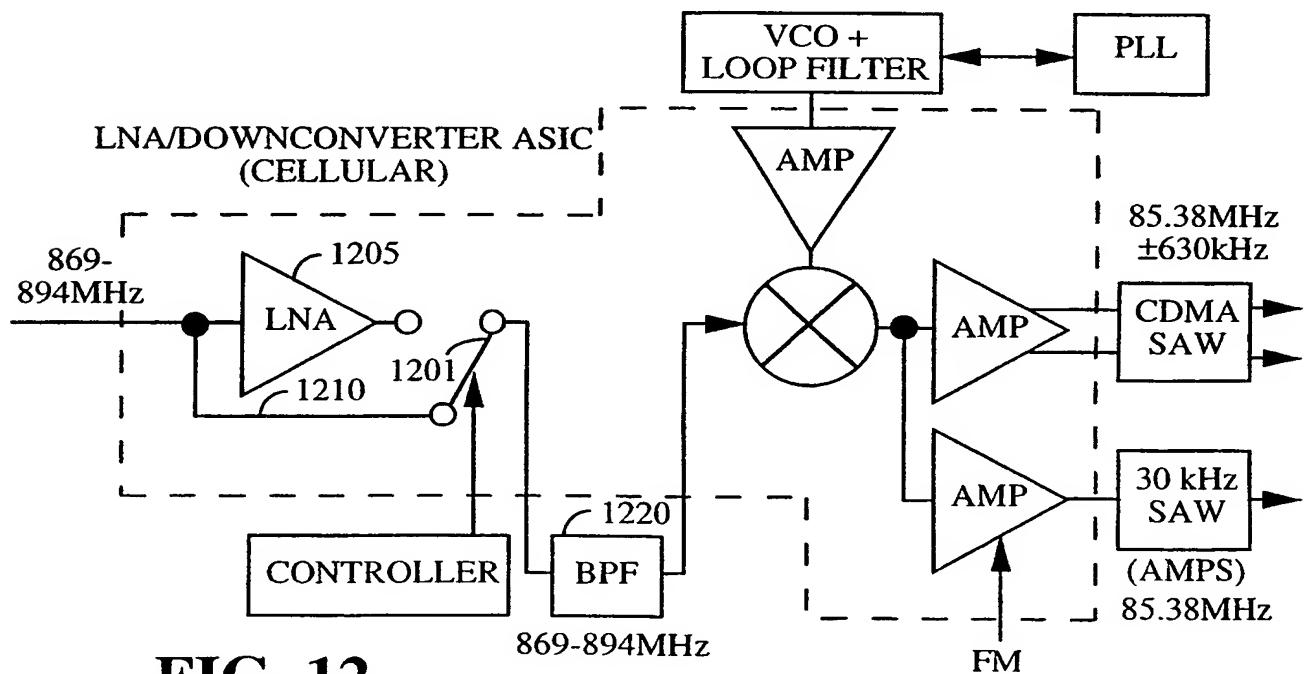


FIG. 9

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**FIG. 11****FIG. 12**

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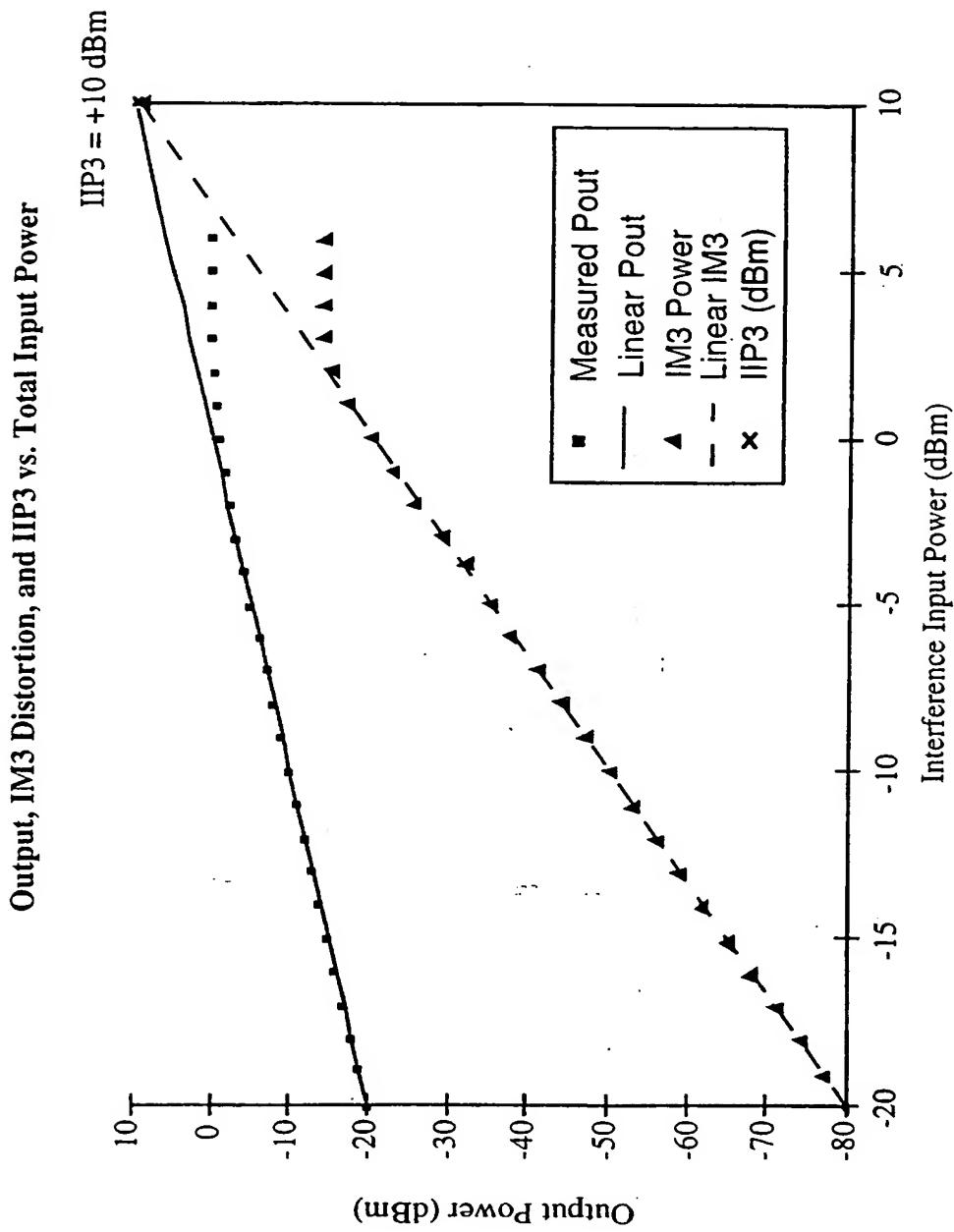
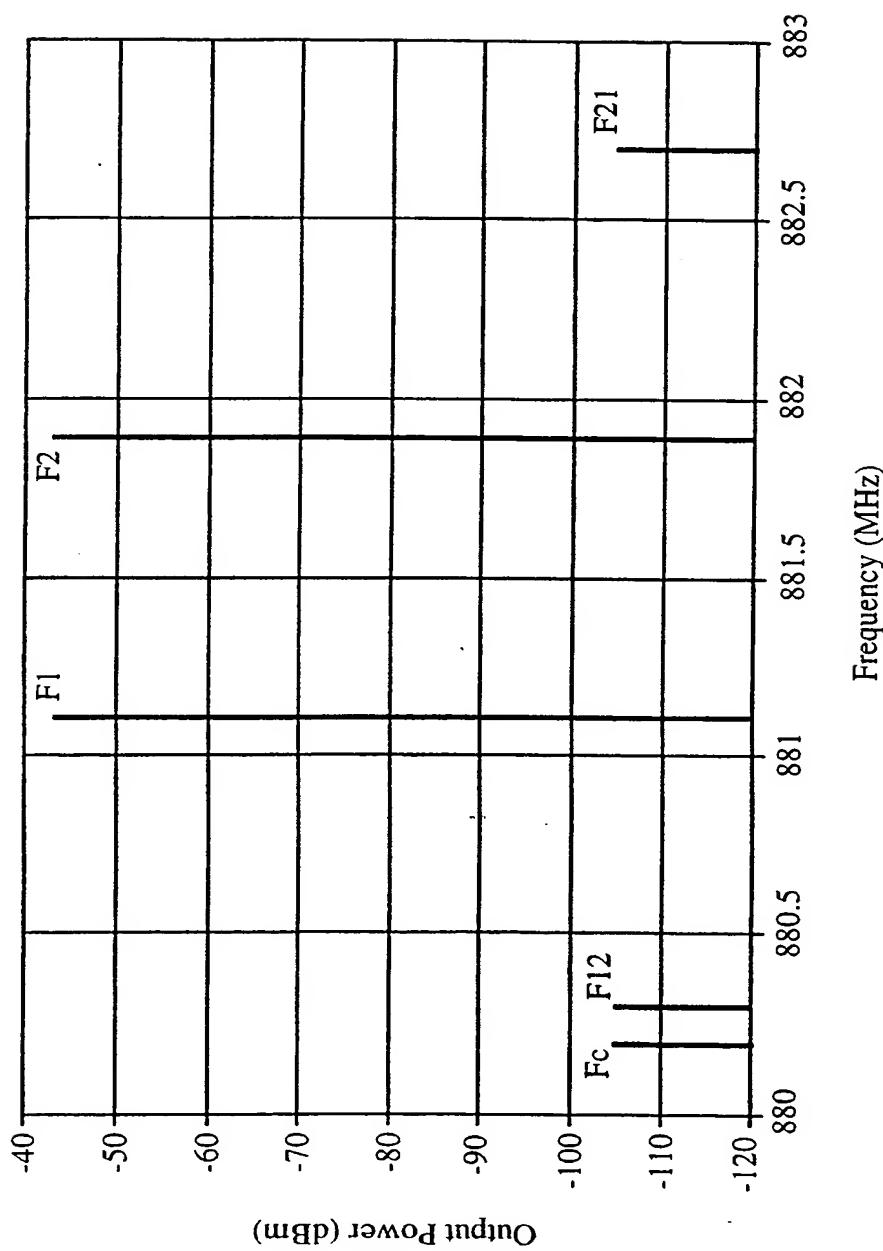


FIG. 13

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**FIG. 14**

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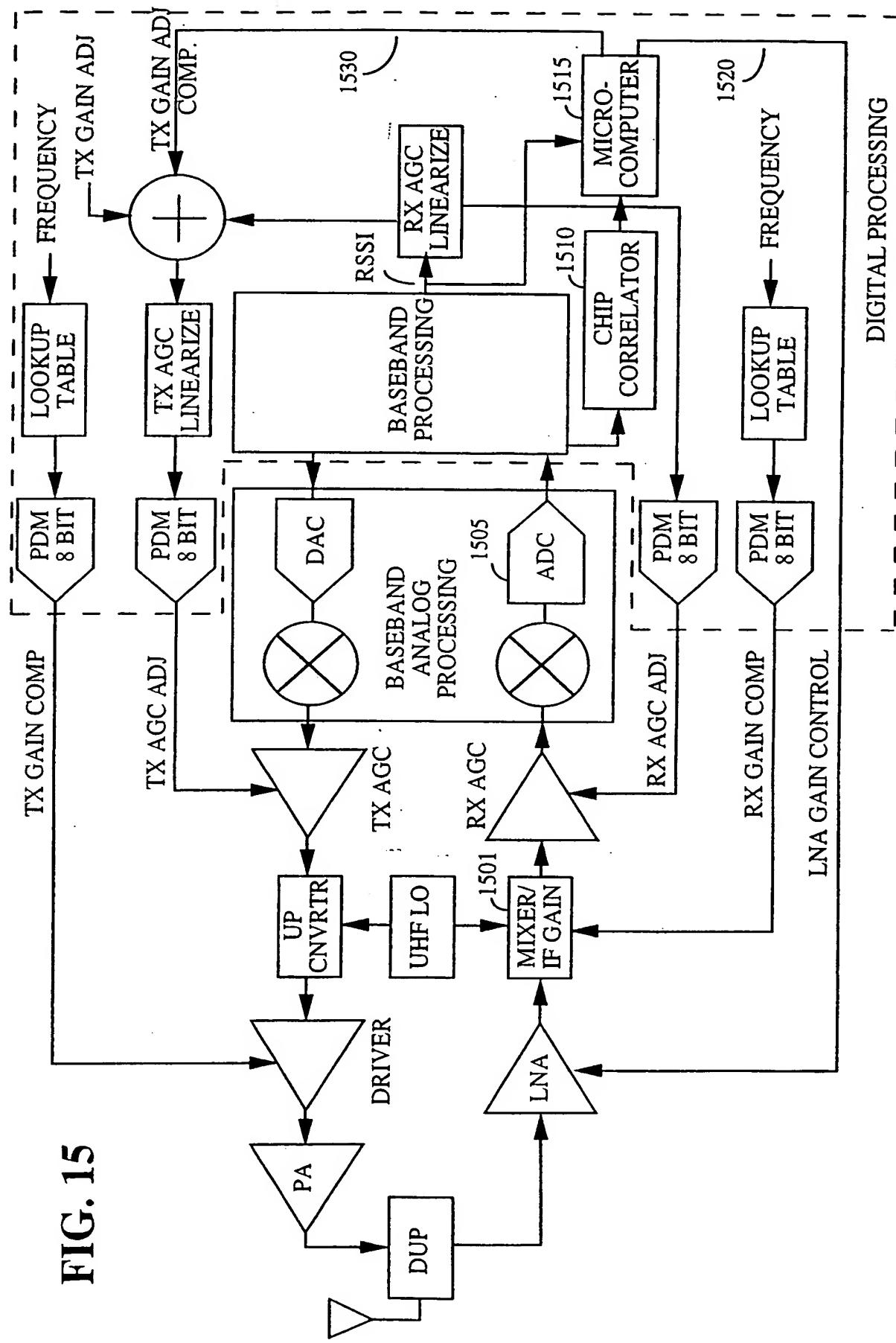
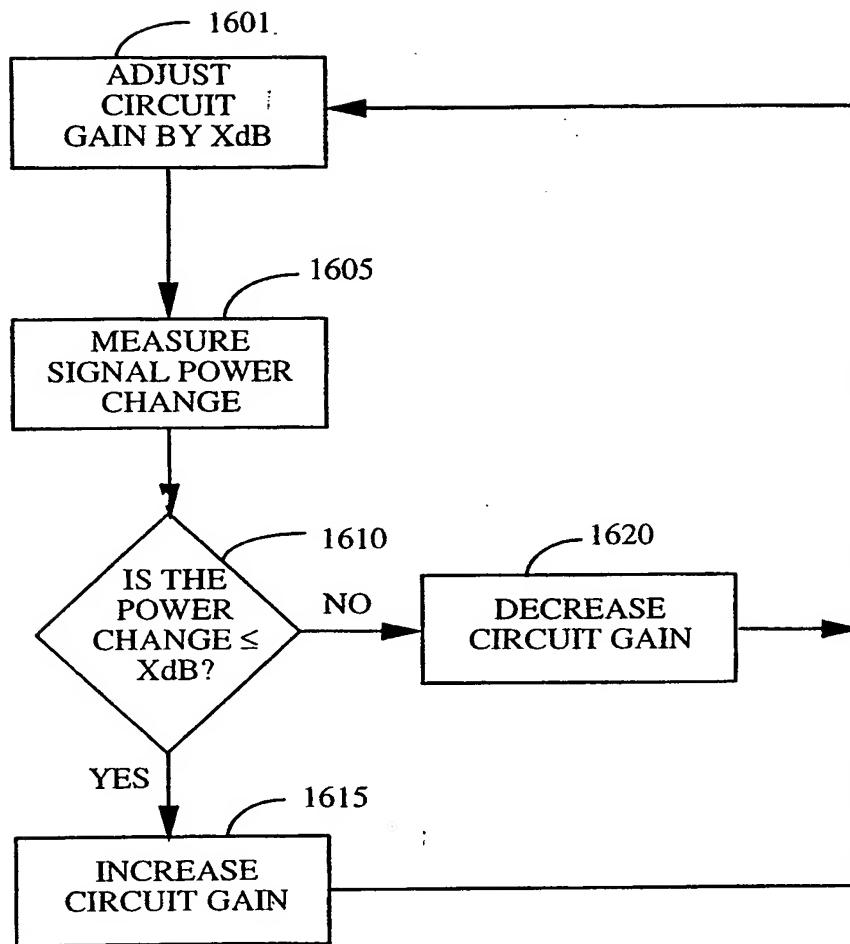


FIG. 15

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**FIG. 16**

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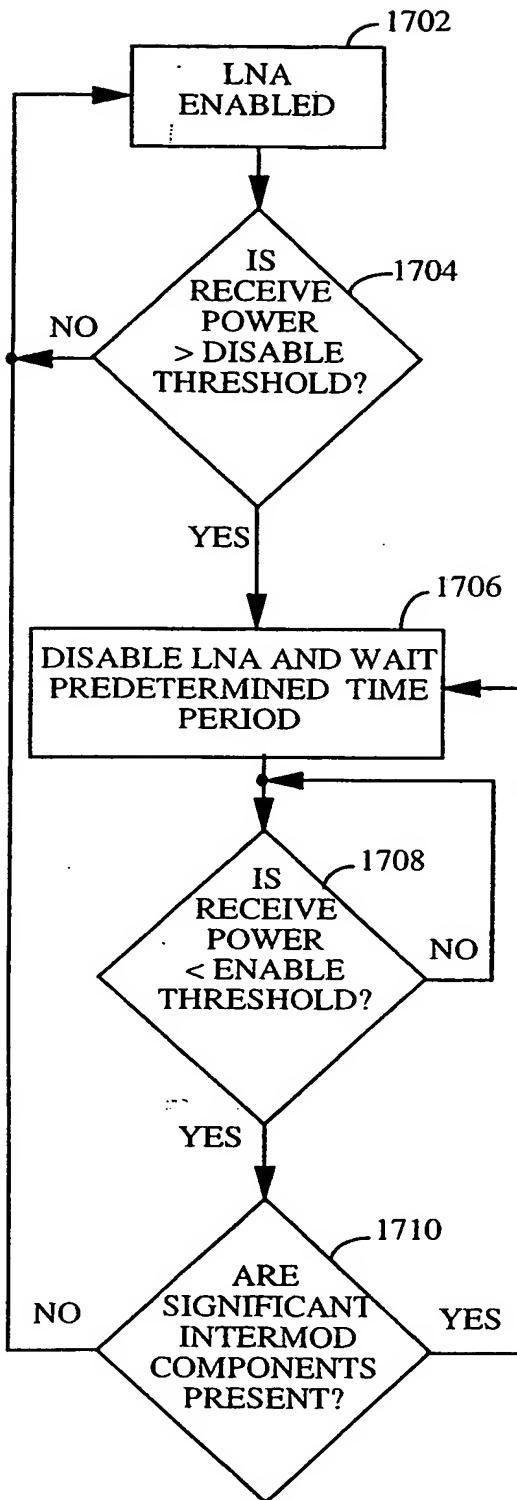


FIG. 17

INTERNATIONAL SEARCH REPORT

International Application No

PCT/US 97/16270

A. CLASSIFICATION OF SUBJECT MATTER

IPC 6 H04B7/005

According to International Patent Classification(IPC) or to both national classification and IPC

B. FIELDS SEARCHED

Minimum documentation searched (classification system followed by classification symbols)

IPC 6 H04B H03G

Documentation searched other than minimum documentation to the extent that such documents are included in the fields searched

Electronic data base consulted during the international search (name of data base and, where practical, search terms used)

C. DOCUMENTS CONSIDERED TO BE RELEVANT

Category	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
A	GB 2 223 146 A (NIPPON ELECTRIC CO) 28 March 1990 see abstract see page 1, line 18 - line 26 see page 2, line 21 - page 3, line 2 see page 6, line 10 - page 7, line 2; figure 1 see page 7, line 17 - page 8, line 18; figures 2,3 --- EP 0 366 485 A (MOTOROLA INC) 2 May 1990 see abstract see page 2, line 10 - line 50 --- -/--	1-3,6,7
A		1,6



Further documents are listed in the continuation of box C.



Patent family members are listed in annex.

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1

Date of the actual completion of the international search

4 February 1998

Date of mailing of the international search report

12/02/1998

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INTERNATIONAL SEARCH REPORT

Int'l. Jonal Application No

PCT/US 97/16270

C.(Continuation) DOCUMENTS CONSIDERED TO BE RELEVANT

Category	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
A	EP 0 342 671 A (AT&T CORPORATION) 23 November 1989 see column 1, line 13 - line 39 see column 2, line 50 - column 3, line 57; figures 1,2 -----	1,6

INTERNATIONAL SEARCH REPORT

Information on patent family members

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